GENERAL DESCRIPTION

The PW2052 is a high efficiency, high frequency synchronous DC-DC step-down regulator. The 100% duty cycle feature provides low dropout operation, extending battery life in portable systems.

The internal synchronous switch increases efficiency and eliminates the need for external Schottky diode. At shutdown mode, the input supply current is less than 1μA. The current limit protection and on-chip thermal shutdown features provide protection against any combination of overload or ambient temperature.

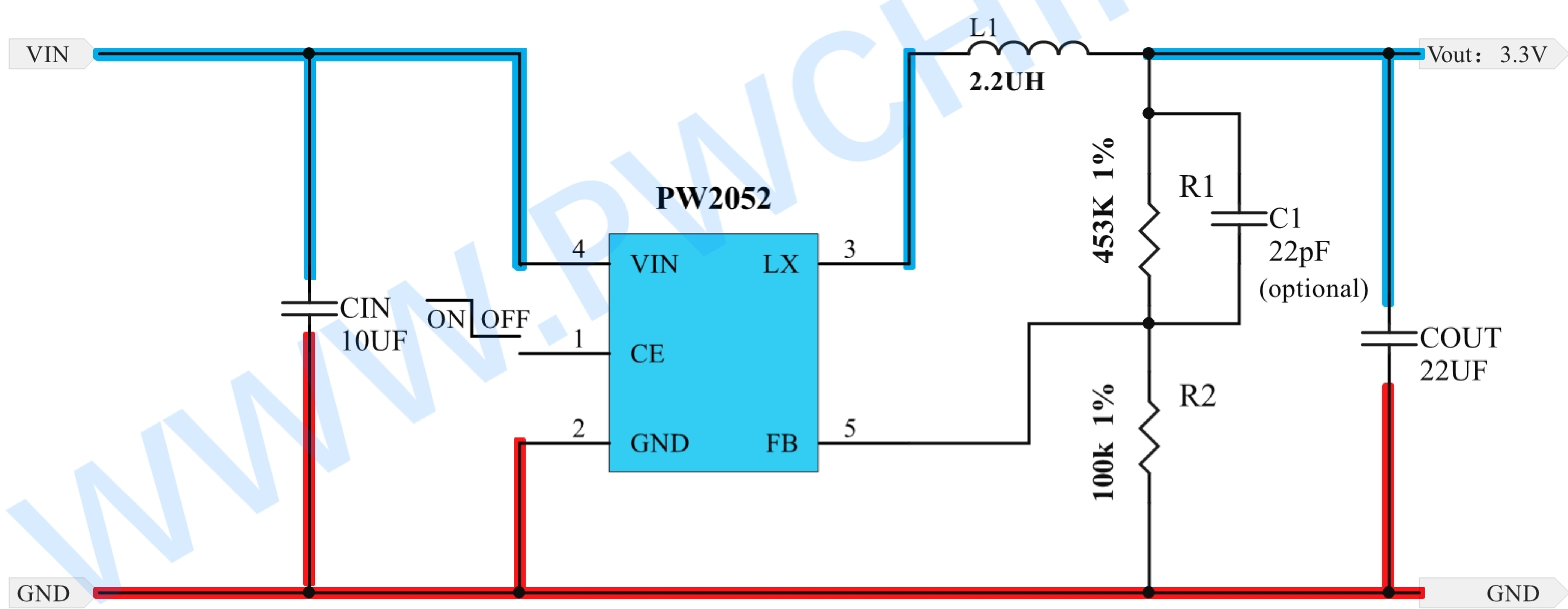
FEATURES

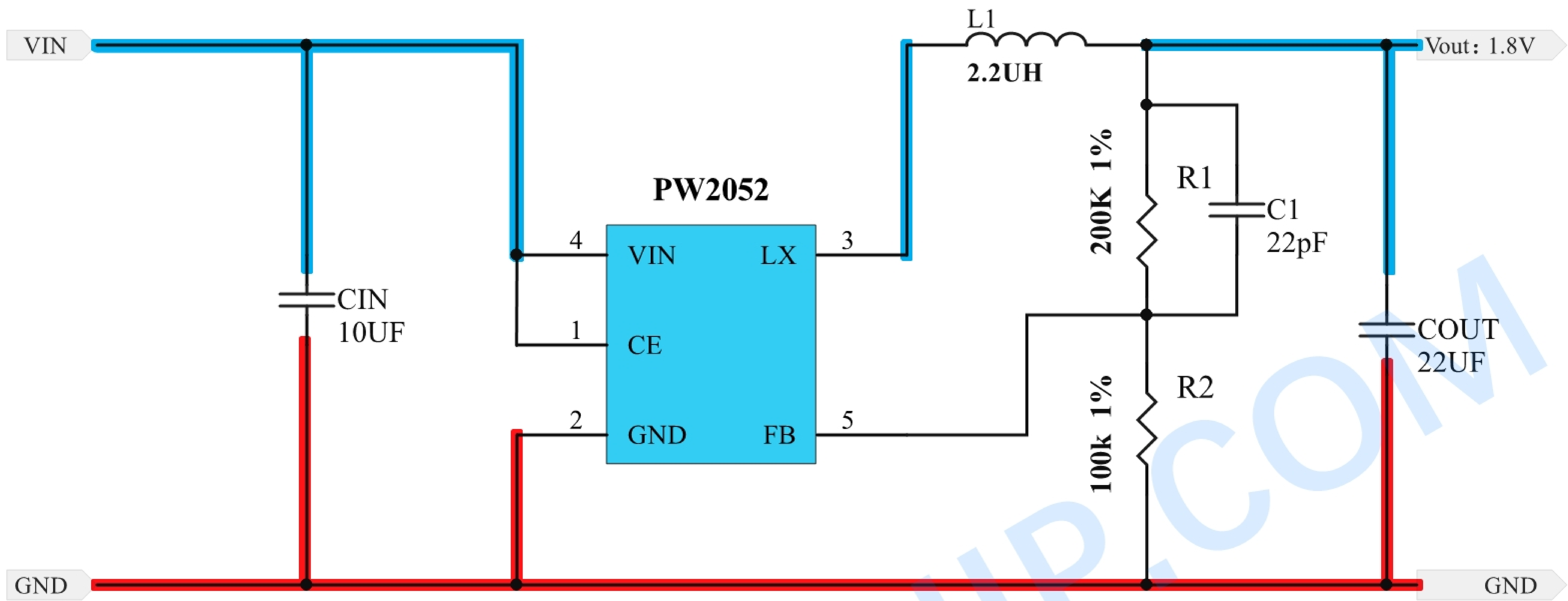
- Low RDS(ON) for Internal Switch (Top/Bottom): 180/100mΩ
- 2.5V~5.5V Input Voltage Range
- 2A Output Current
- 1MHz Switching Frequency Minimizes the External Components
- Internal Soft-Start Limits the Inrush Current
- Internal Compensation Function
- 100% Dropout Operation
- RoHS Compliant and Halogen Free
- SOT-23-5 Packages

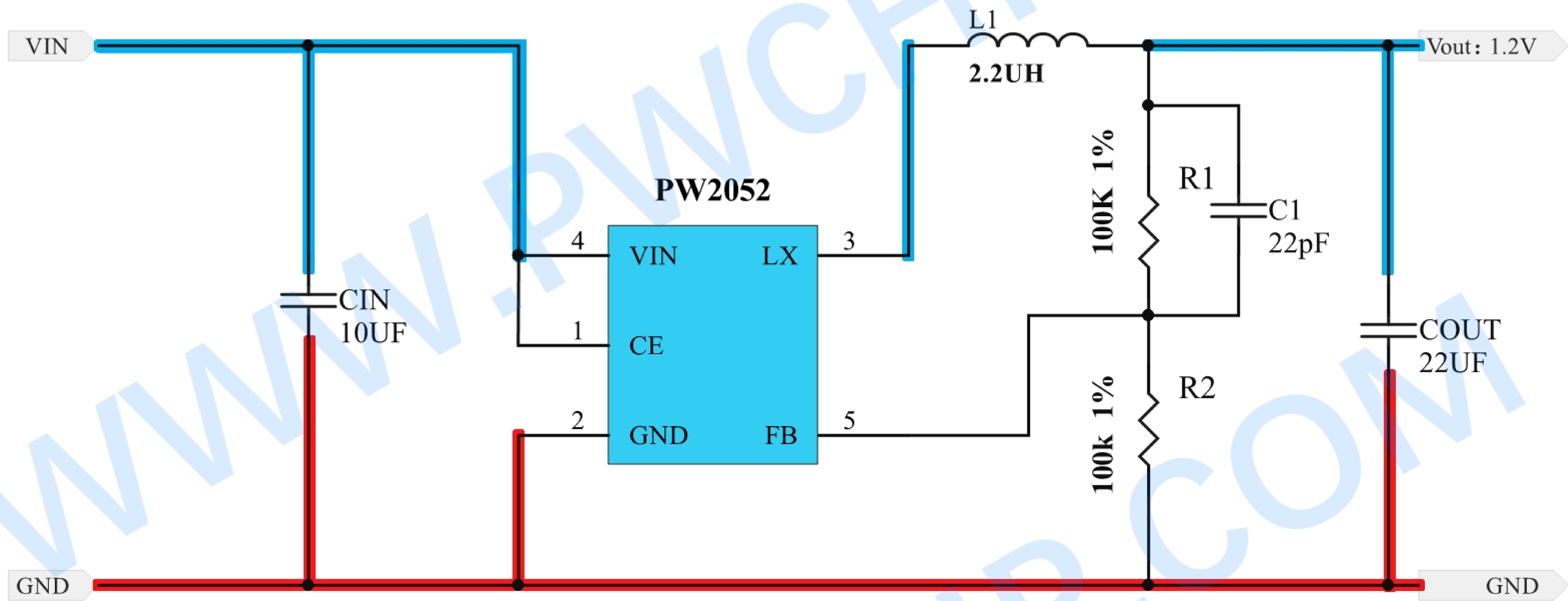
APPLICATIONS

- Set Top Box
- LCD TV
- Tablet
- Portable Equipment

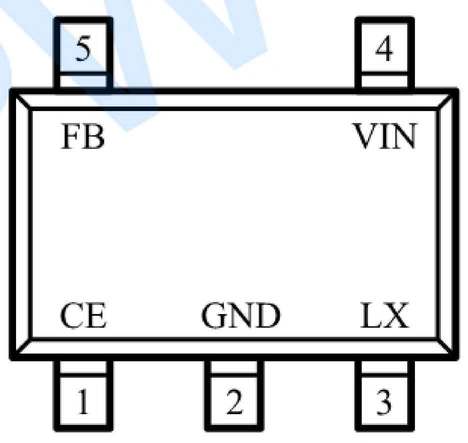
TYPICAL APPLICATION CIRCUIT







PIN ASSIGNMENT/DESCRIPTION



SOT-23-5L
(TOP VIEW)

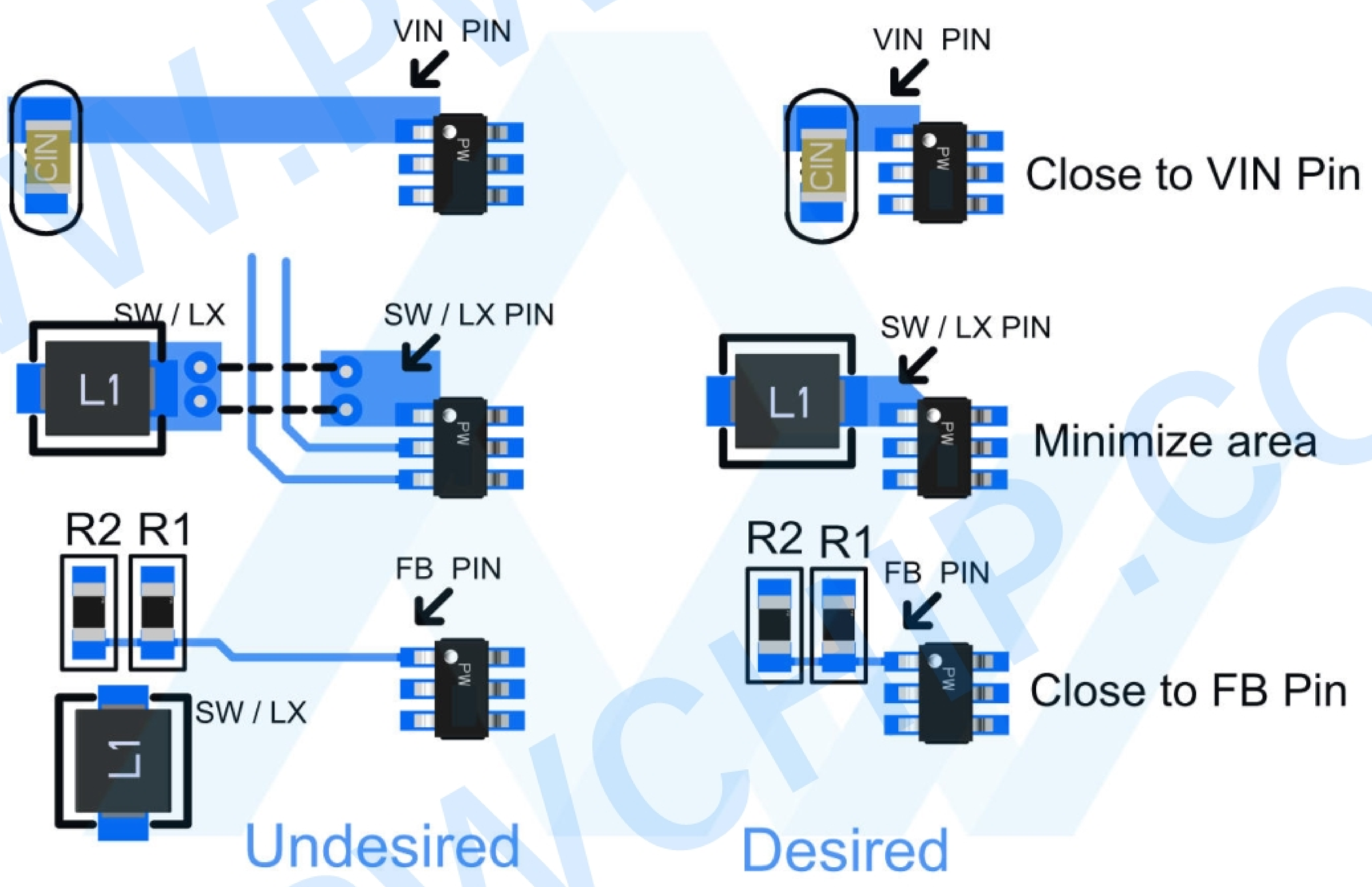
Pin Number	Pin Name	Function
1	CE	Enable Control. Pull high to turn the IC on, and pull low to disable the IC.
2	GND	Ground Pin.
3	LX	Power Switching Node. Connect an inductor to the drains of internal high side PMOS and low side NMOS
4	VIN	Power Supply Input Pin. Place input capacitors as close as possible from VIN to GND to avoid noise influence.
5	FB	Voltage Feedback Input Pin. Connect FB and VOUT with a resistive voltage divider.This IC senses feedback voltage via FB and regulates it at 0.6V.

PCB Layout Recommendation

The device's performance and stability are dramatically affected by PCB layout. It is recommended to follow these general guidelines shown as below:

1. Place the input capacitors and output capacitors as close to the device as possible. The traces which connect to these capacitors should be as short and wide as possible to minimize parasitic inductance and resistance.
2. Place feedback resistors close to the FB pin.
3. Keep the sensitive signal (FB) away from the switching signal (LX).
4. Multi-layer PCB design is recommended.

PCB layout



Products

<table>
<tr><th>Reel /outer anti-static packaging</th><th colspan="2">Product</th></tr>
<tr><td rowspan="8">

NO： 1, QR code content: WWW.PWCHIP.COM;
2. Product: PWCHIP product model name;
3. Lot No: wafer batch code/internal system production code (customers can send this code to support@pwchip.com to verify product information and confirm);
4. D/C: packaging cycle;
5. QTY: packaging quantity (box/disc);
6. Data: packaging time.</td><td colspan="2">PW2052</td></tr>
<tr><th>Brand</th><th>Package</th></tr>
<tr><td>平芯微/PWCHIP</td><td>SOT23-5L</td></tr>
<tr><th>Specification</th><th>Qty per reel</th></tr>
<tr><td>Taping & Reel</td><td>3000 PCS</td></tr>
<tr><th colspan="2">Marking</th></tr>
<tr><td colspan="2">fiwXXX
Device code: fiw； Lot number code: XXX</td></tr>
</table>

Absolute Maximum Ratings (note1)

- VIN to GND -- -0.3V to +6.5V
- LX to GND --- -0.3V to VIN+0.3V
- CE, FB, to GND -- -0.3V to VIN
- Package Thermal esistance, (θJA) -- ----------------------- +250ºC/W
- Package Thermal esistance, (θJC)-------------------------- +130°C/W
- Maximum Junction Temperature (TJ) ------------------------ +150°C
- Lead Temperature (Soldering, 10 sec.) ----------------------- +260°C
- Storage Temperature (TSTG) -------------------------------- -65°C to +150℃

Note 1： Stresses beyond those listed under "Absolute Maximum atings" may cause permanent damage to the device

Recommended Operating Conditions (Note 2)

- Supply Voltage (VIN) -------------------------------------- +2.5V to +5.5V
- Junction Temperature Range -------------------------------- -40°C to +125°C
- Ambient Temperature Range --------------------------------- -40°C to +85°C

Note 2： The device is not guaranteed to function outside its operating conditions.

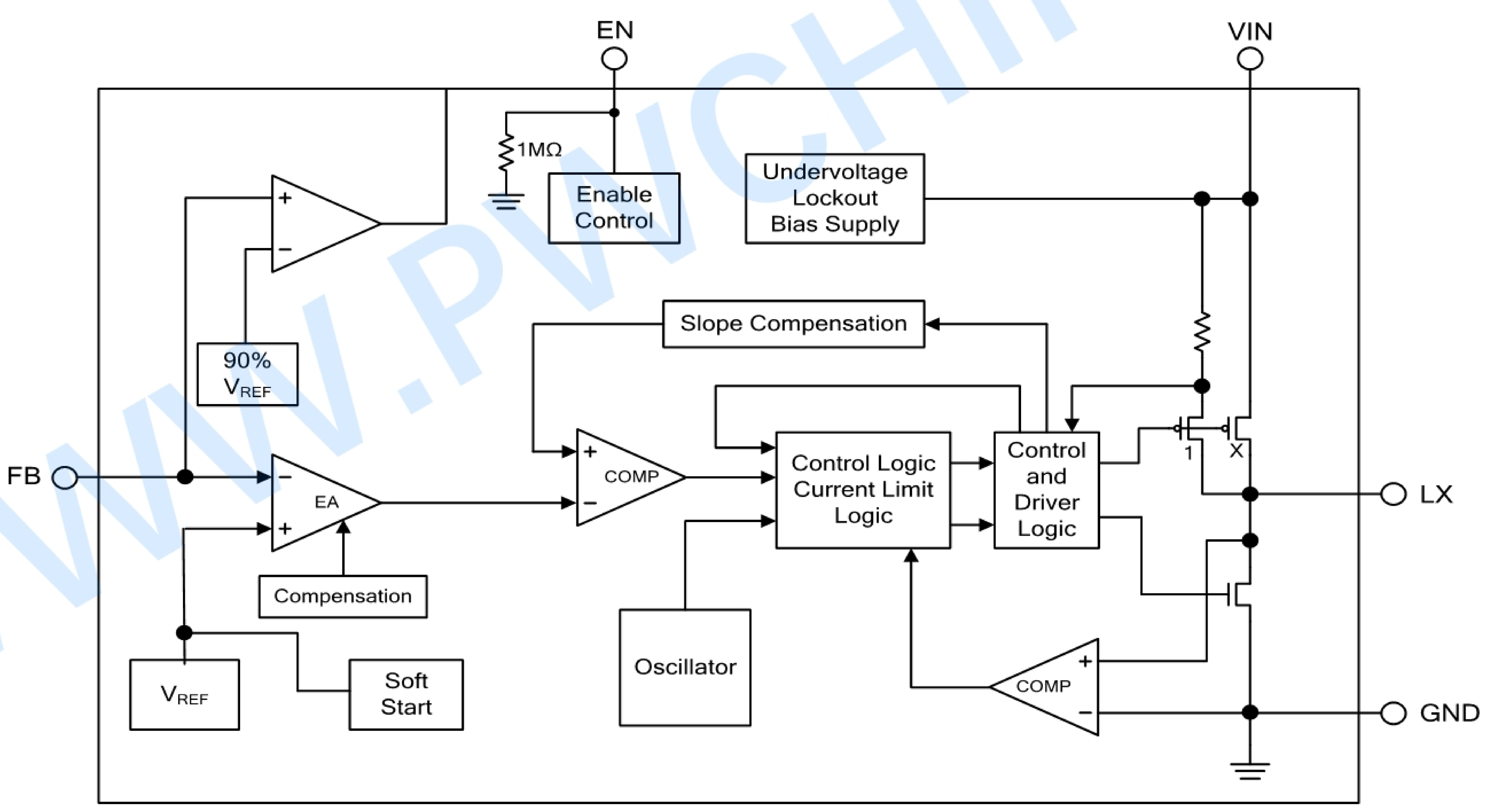
ELECTRICAL CHARACTERISTICS

(VIN=5V, TA=25°C, unless otherwise specified.)

Parameter	Symbol	Conditions	Min	Typ	Max	Unit
Shutdown Current	I_{SHDN}	CE=GND		0.1	1	μA
Quiescent Current	I_q	V_{FB}=0.65V, I_{OUT}=0A		80		μA
Reference Voltage	V_{REF}		0.588	0.6	0.612	V
FB Input Leakage Current	I_{FB}	$V_{FB}=V_{IN}$		0.01	1	μA
P-Channel MOSFET On-Resistance (Note 3)	$R_{DS(ON)}$			180		mΩ
N-Channel MOSFET On-Resistance (Note 3)	$R_{DS(ON)}$			100		mΩ
P-Channel Current Limit (Note 3)	I_{LIM}		2.2	2.7		A
CE High-Level Input Voltage	V_{IH}		1.5			V
CE Low-Level Input Voltage	V_{IL}				0.4	V
Under Voltage Lockout Voltage	UVLO			2.4		V
UVLO Hysteresis	V_{HYS}			0.2		V
Oscillation Frequency	F_{OSC}	I_{OUT}=500mA	0.8	1	1.2	MHz
Minimum On Time				50		ns
Maximum Duty Cycle			100			%
VOUT Discharge Resistance				100		Ω
Thermal Shutdown Temperature (Note 3)	T_{SD}			150		°C
Internal Soft Start Time	T_{SS}			1		ms

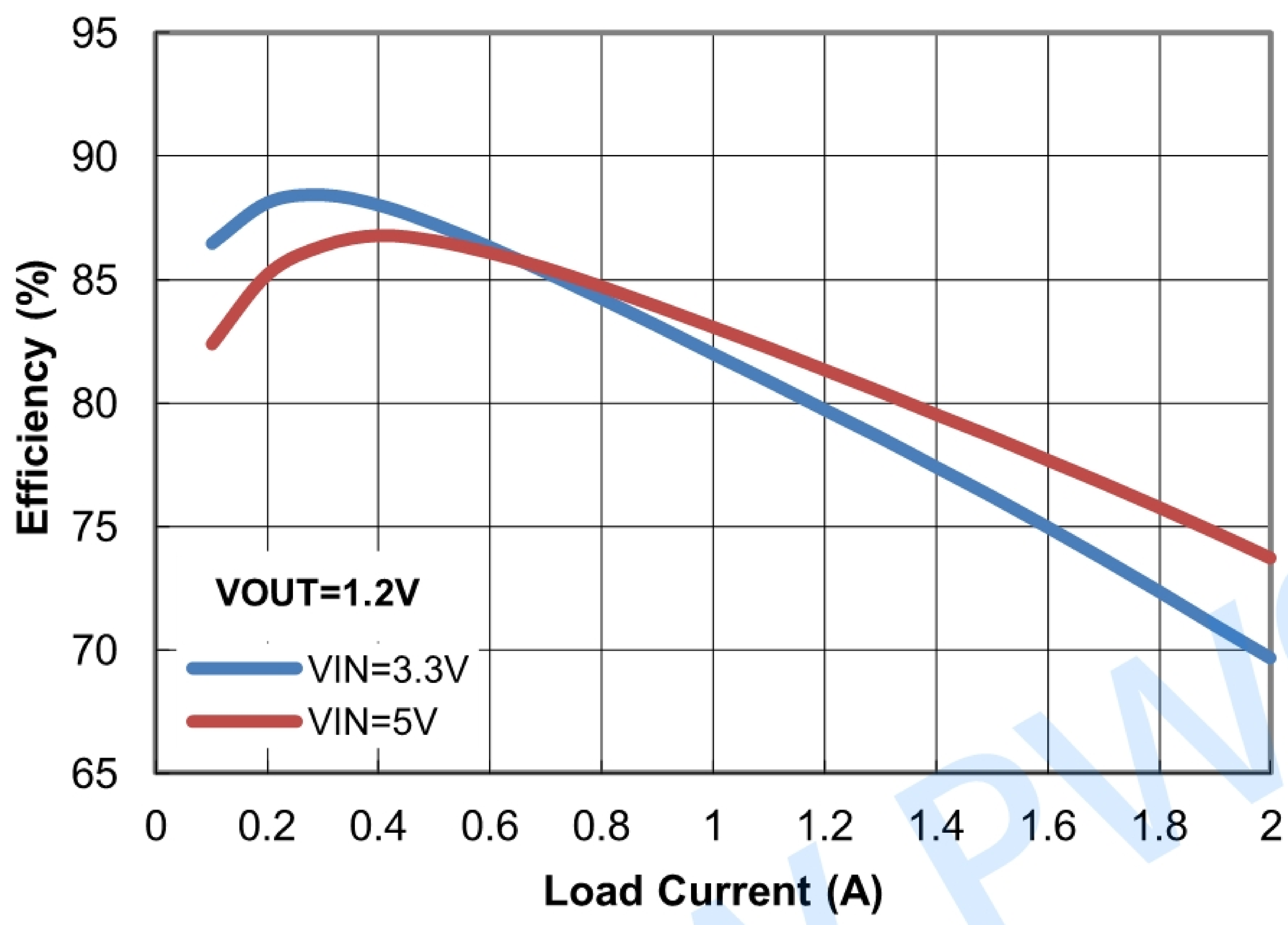
Note 3：Guarantee by design.

Block Diagram

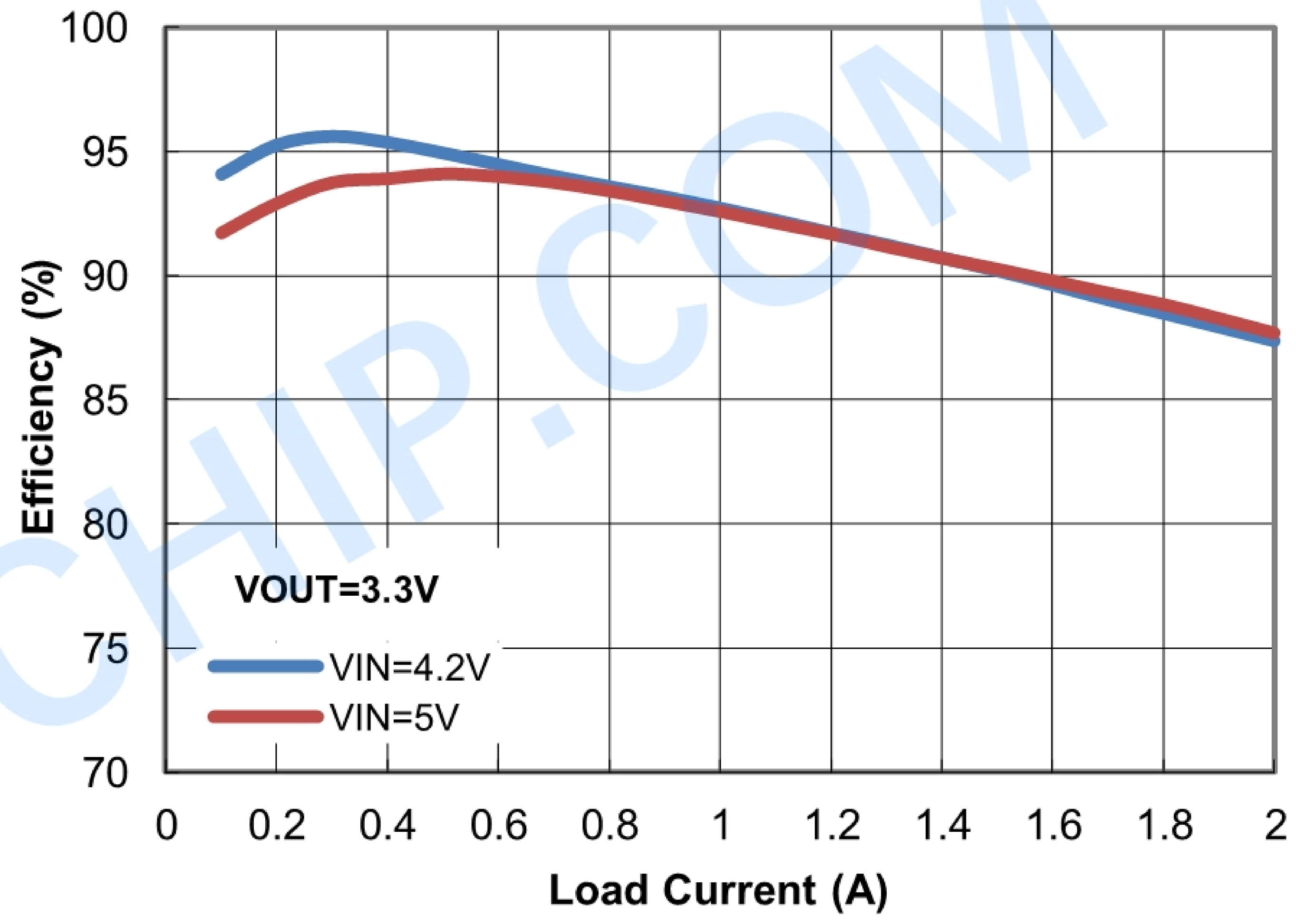


Typical Performance Curves

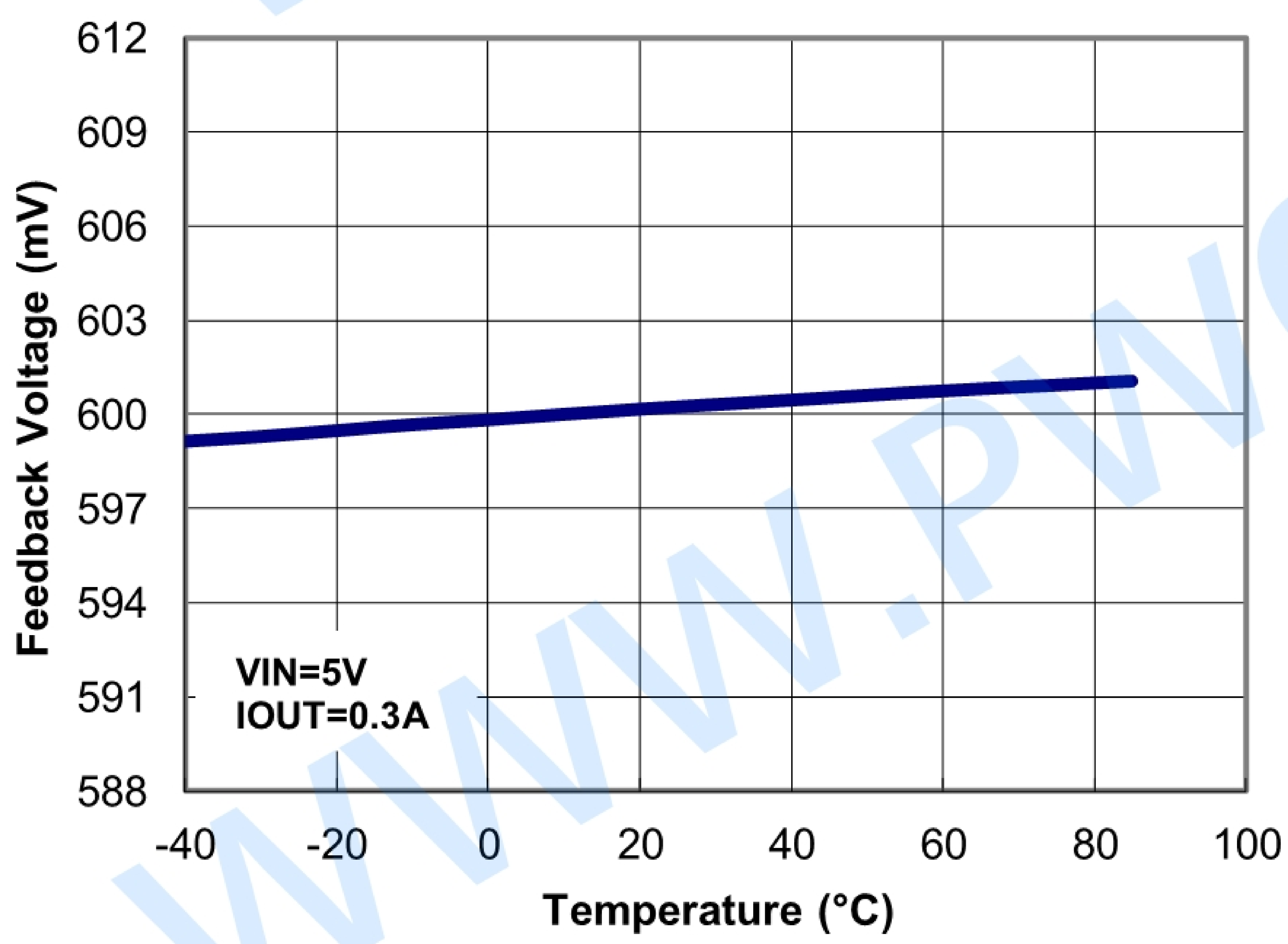
(VIN=5V, VOUT=1.2V , CIN=10μF, COUT=10 μF, L1=1.5μH, TA=25°C, unless otherwise noted.)



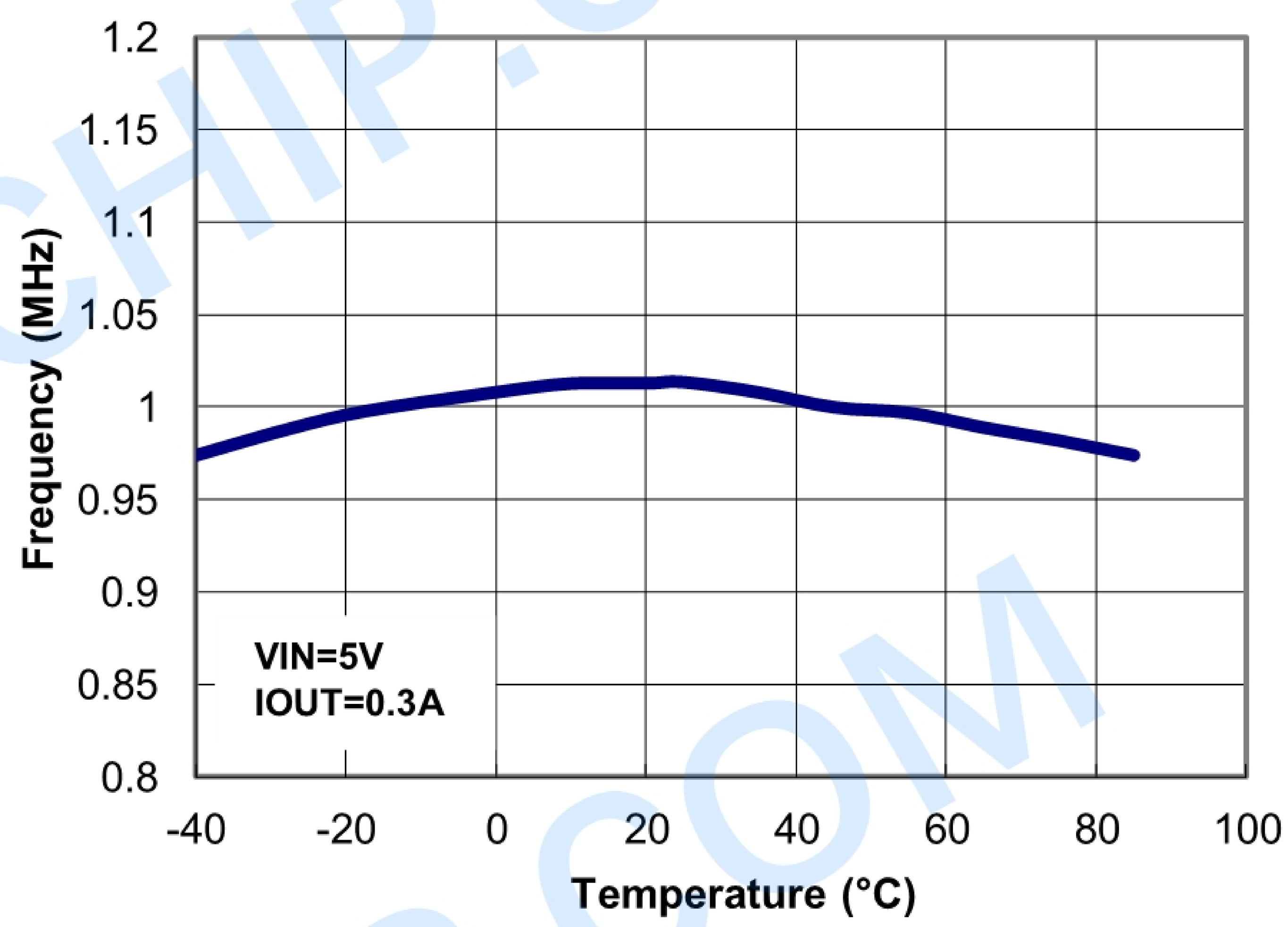
Efficiency vs. Load Current



Efficiency vs. Load Current

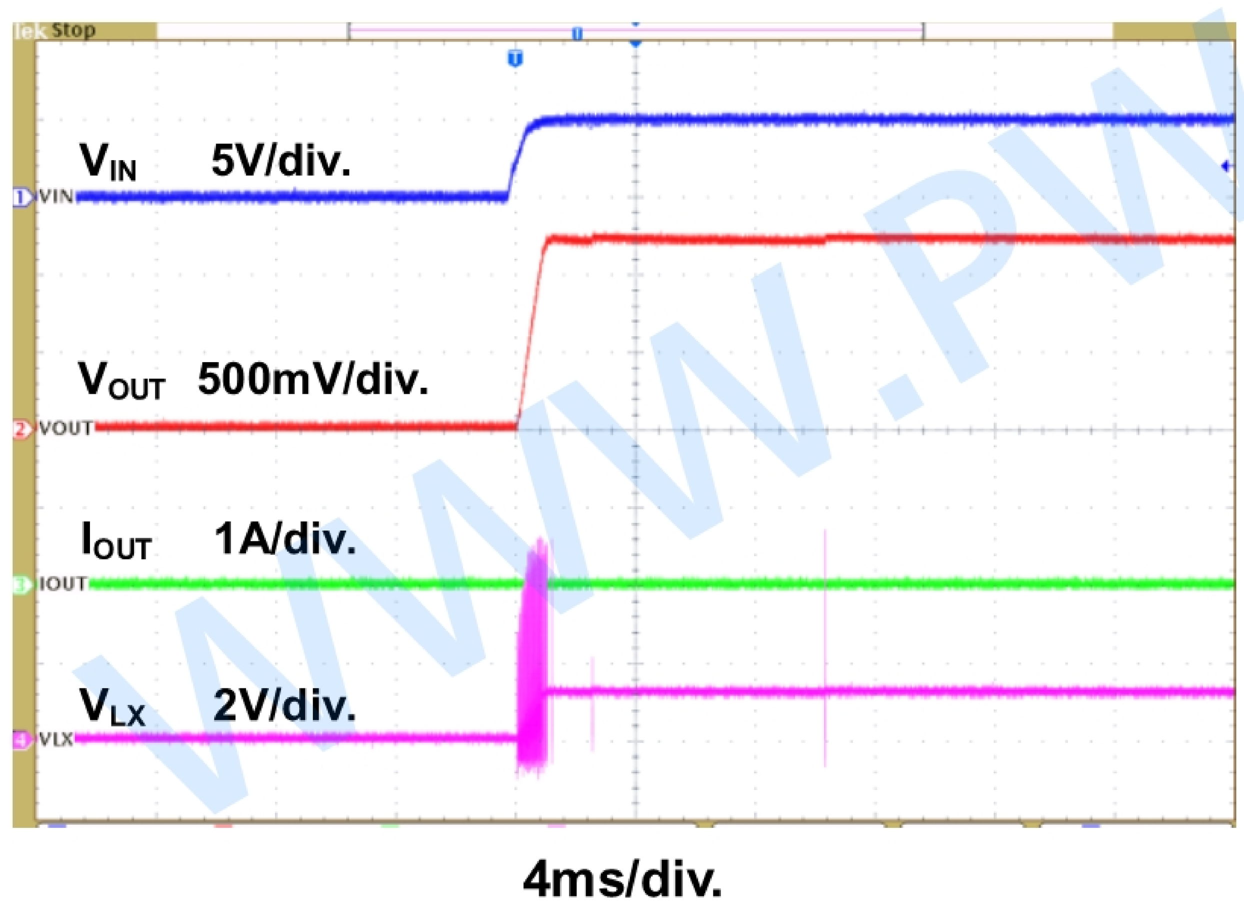


Feedback Voltage vs. Temperature



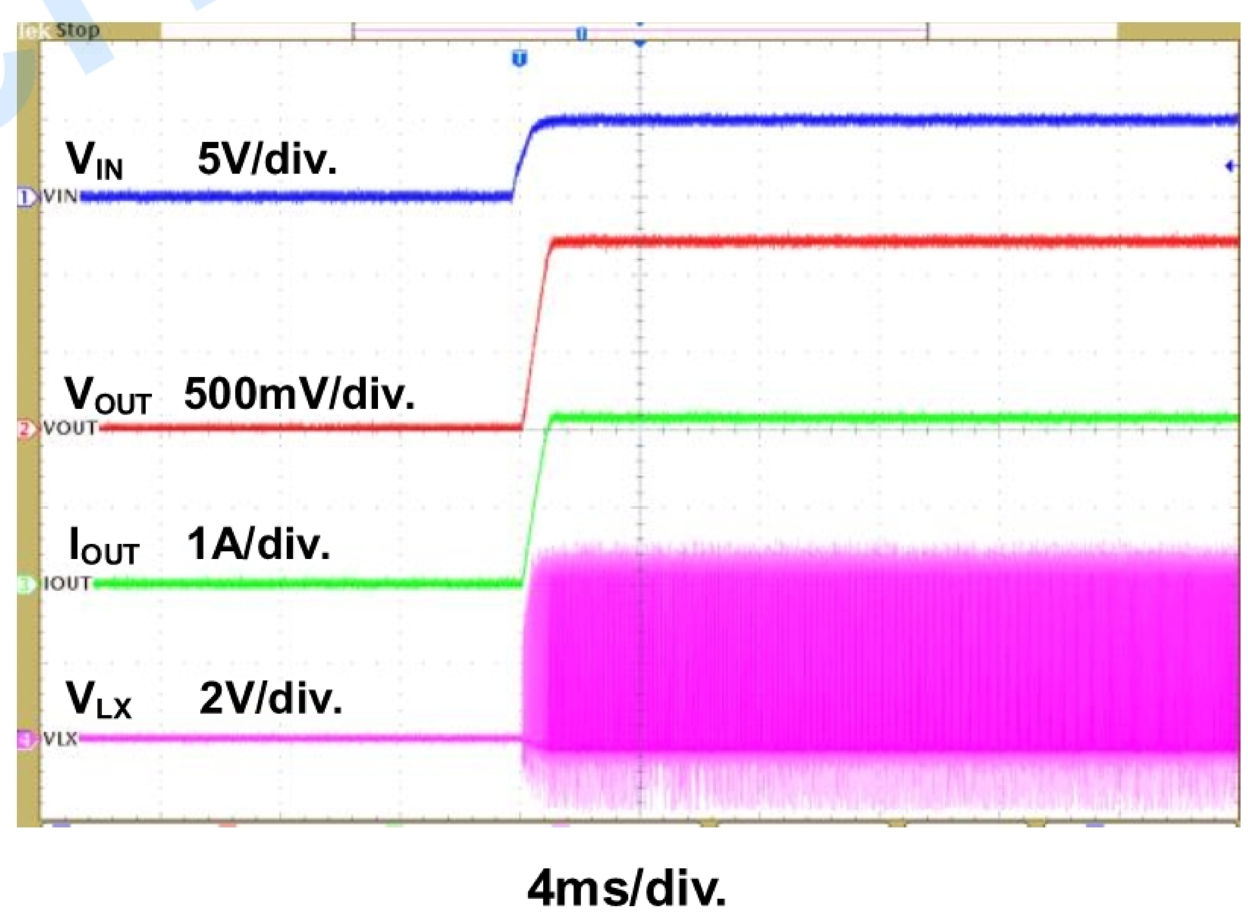
Frequency vs. Temperature

I_{OUT}=0A



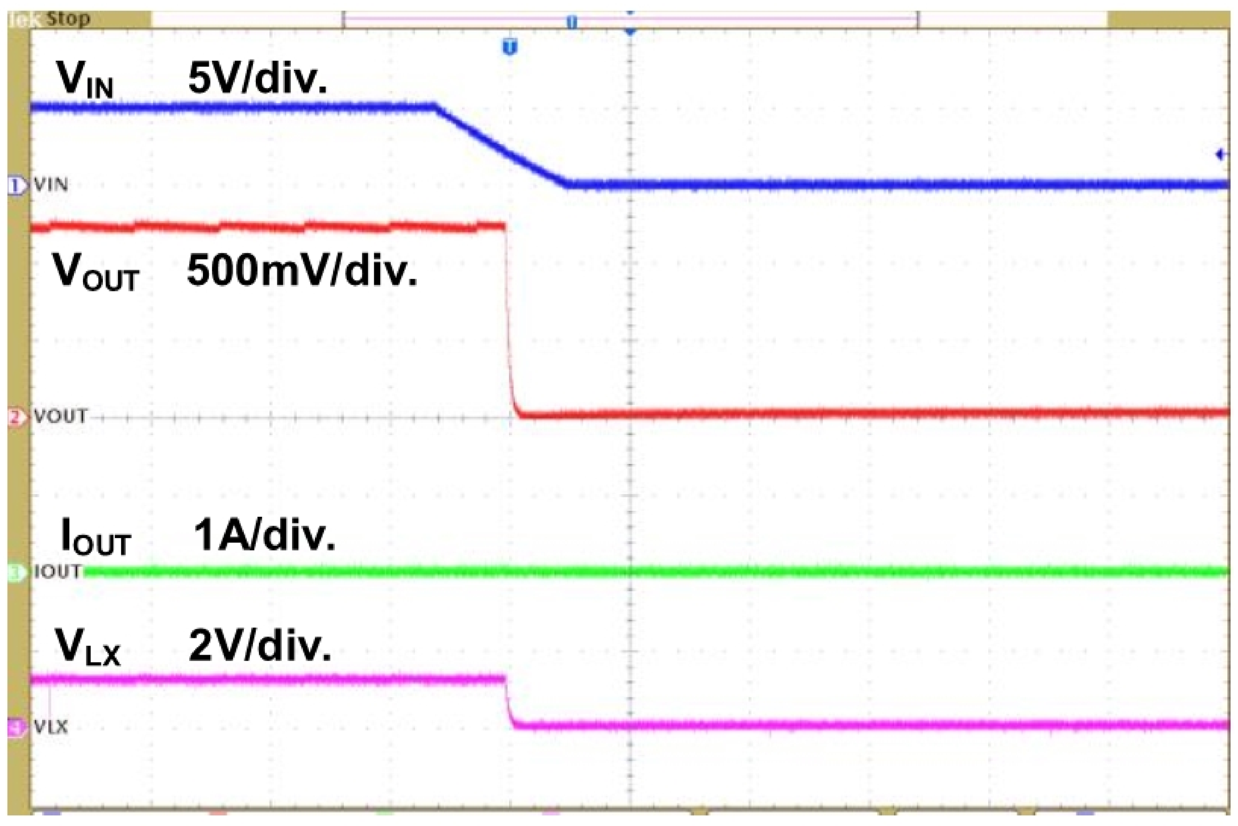
Power On through VIN Waveform

I_{OUT}=2A



Power On through VIN Waveform

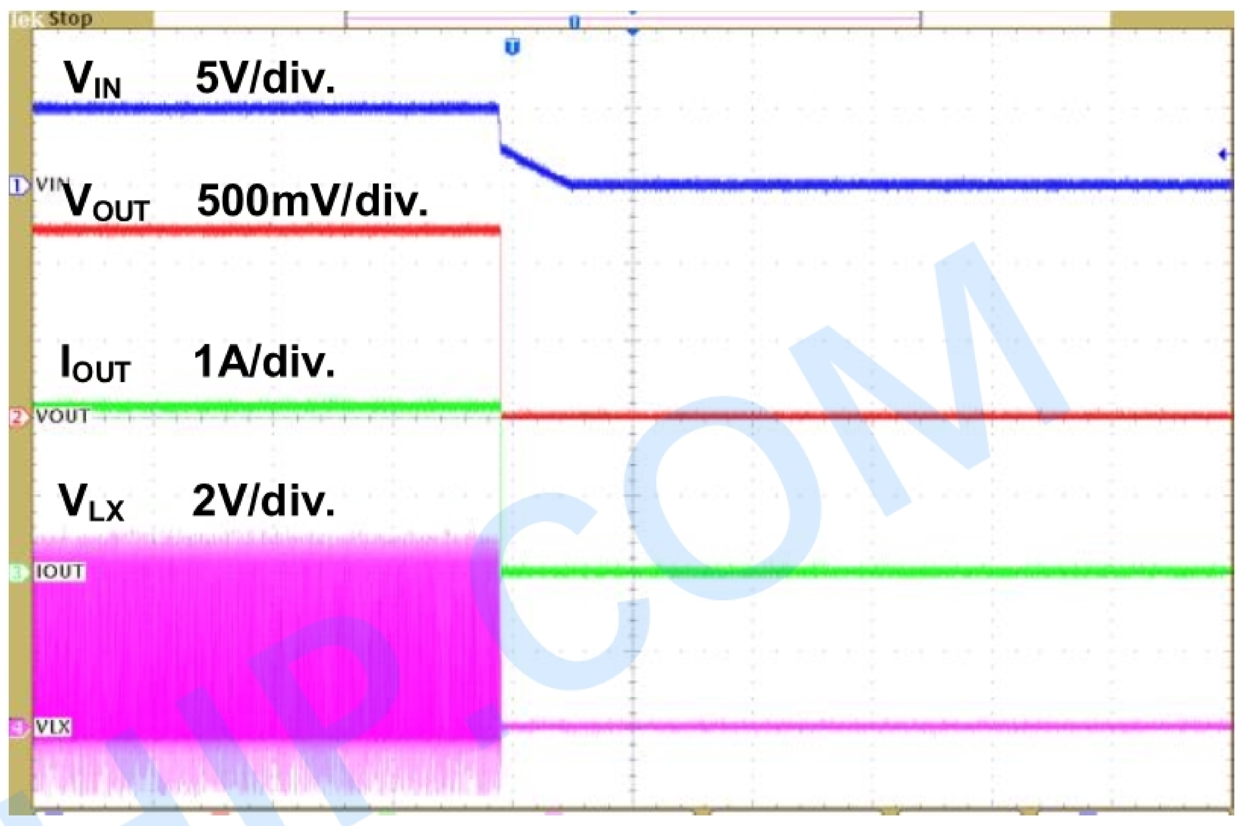
I_{OUT}=0A



100ms/div.

Power Off through VIN Waveform

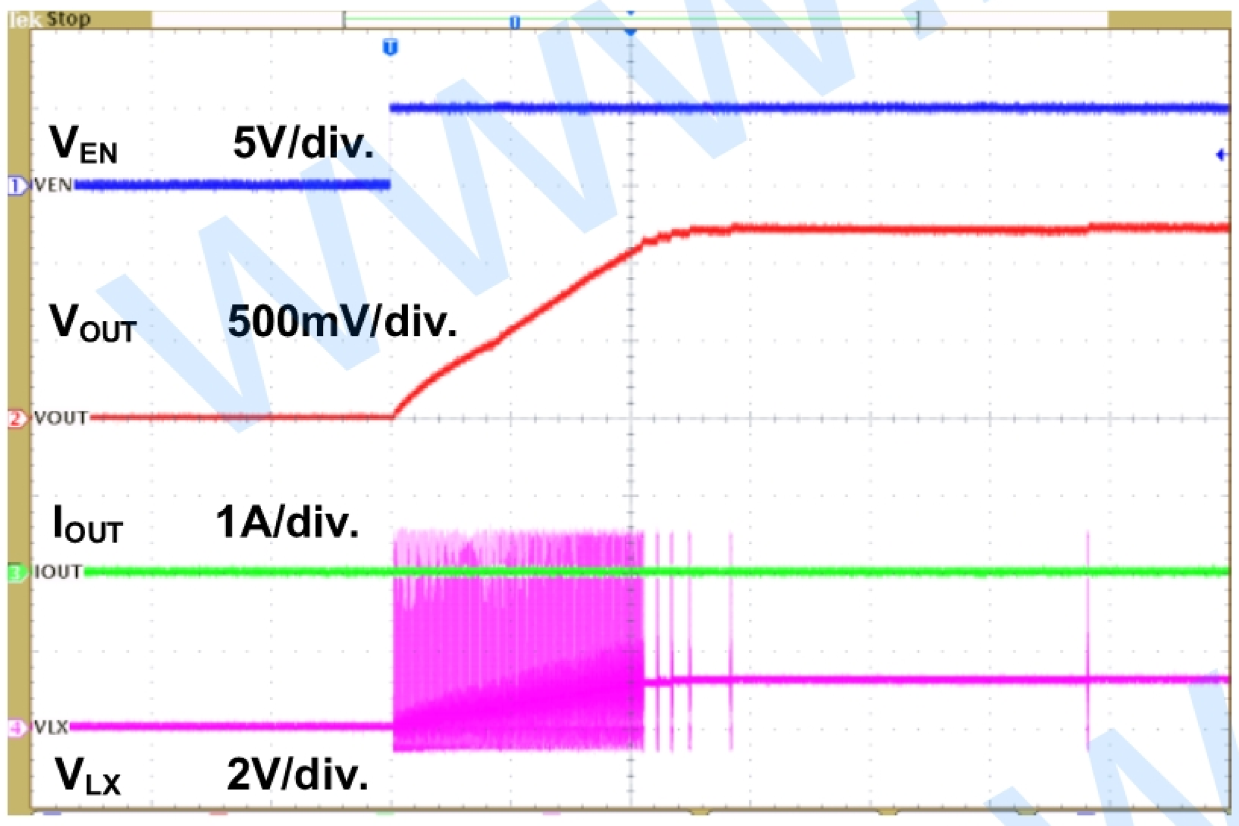
I_{OUT}=2A



100ms/div.

Power Off through VIN Waveform

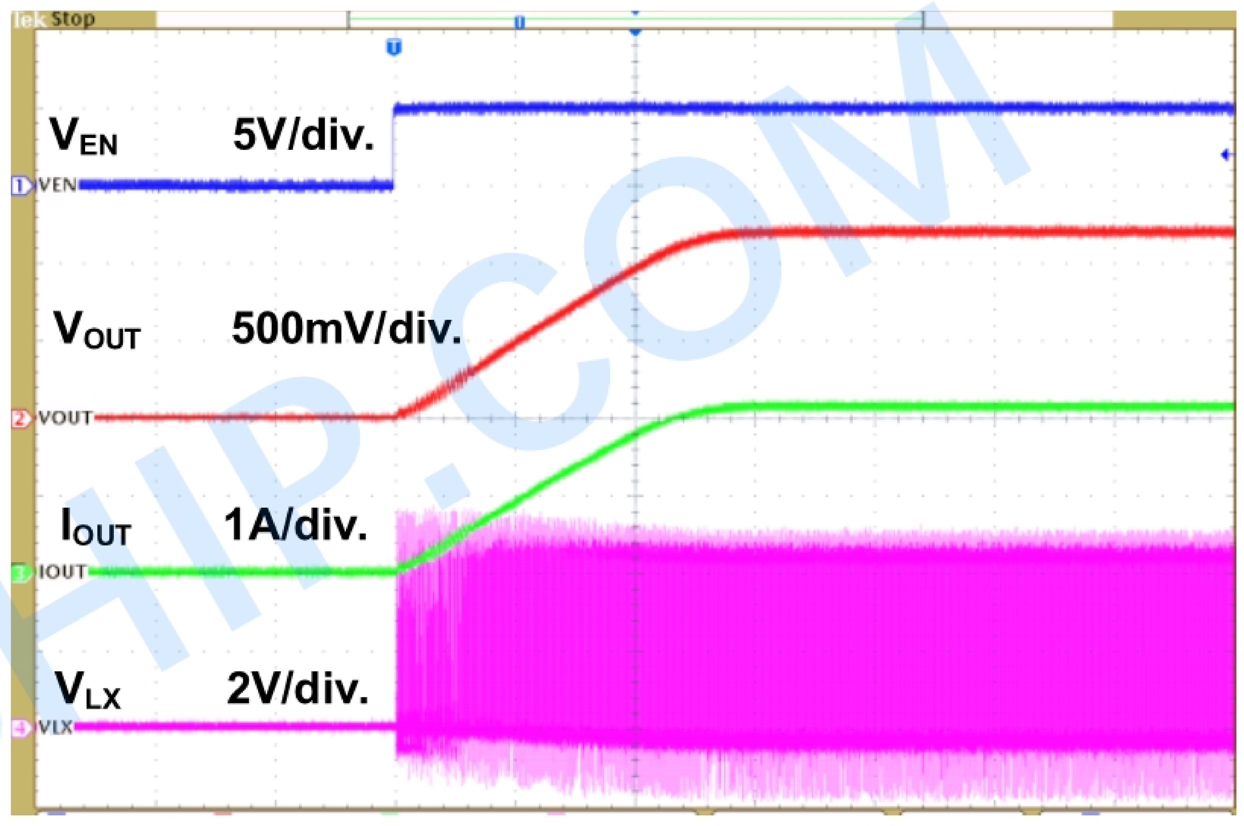
I_{OUT}=0A



400μs/div.

Power On through EN Waveform

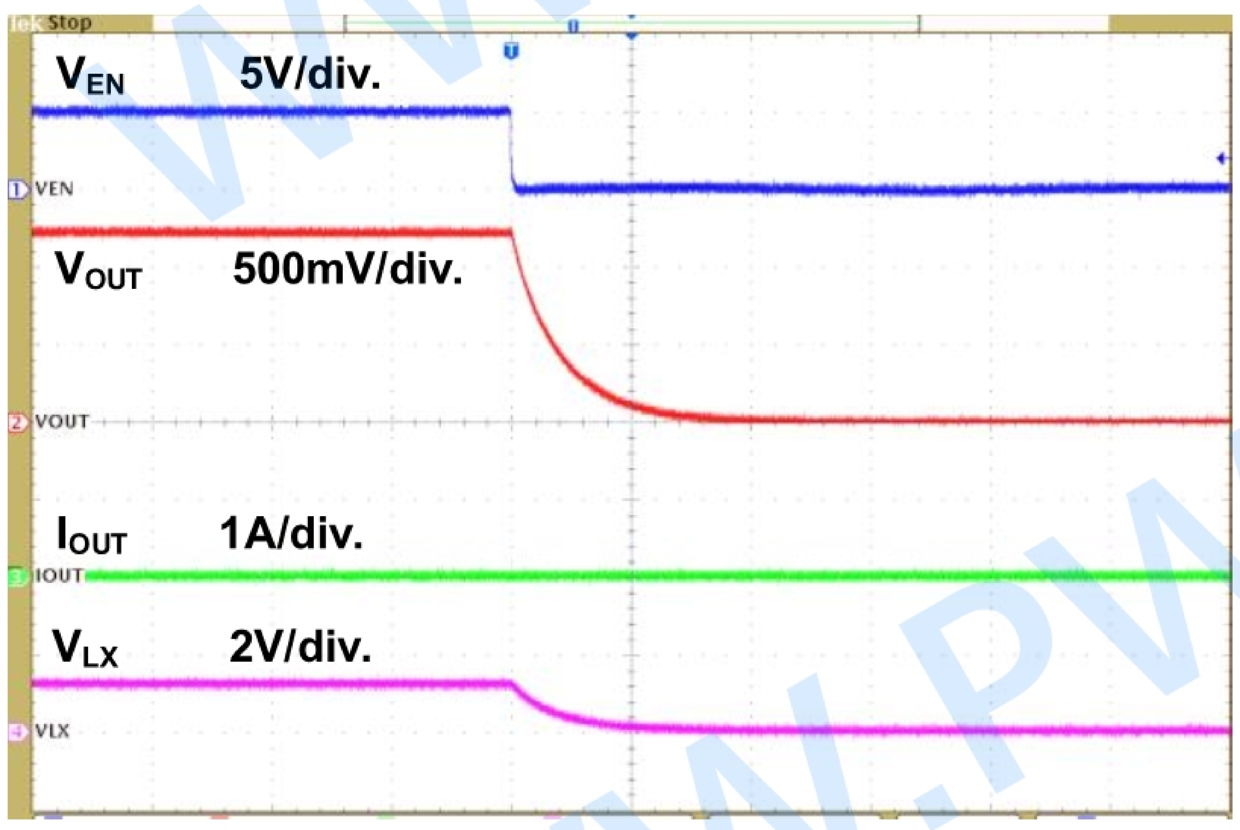
I_{OUT}=2A



400μs/div.

Power On through EN Waveform

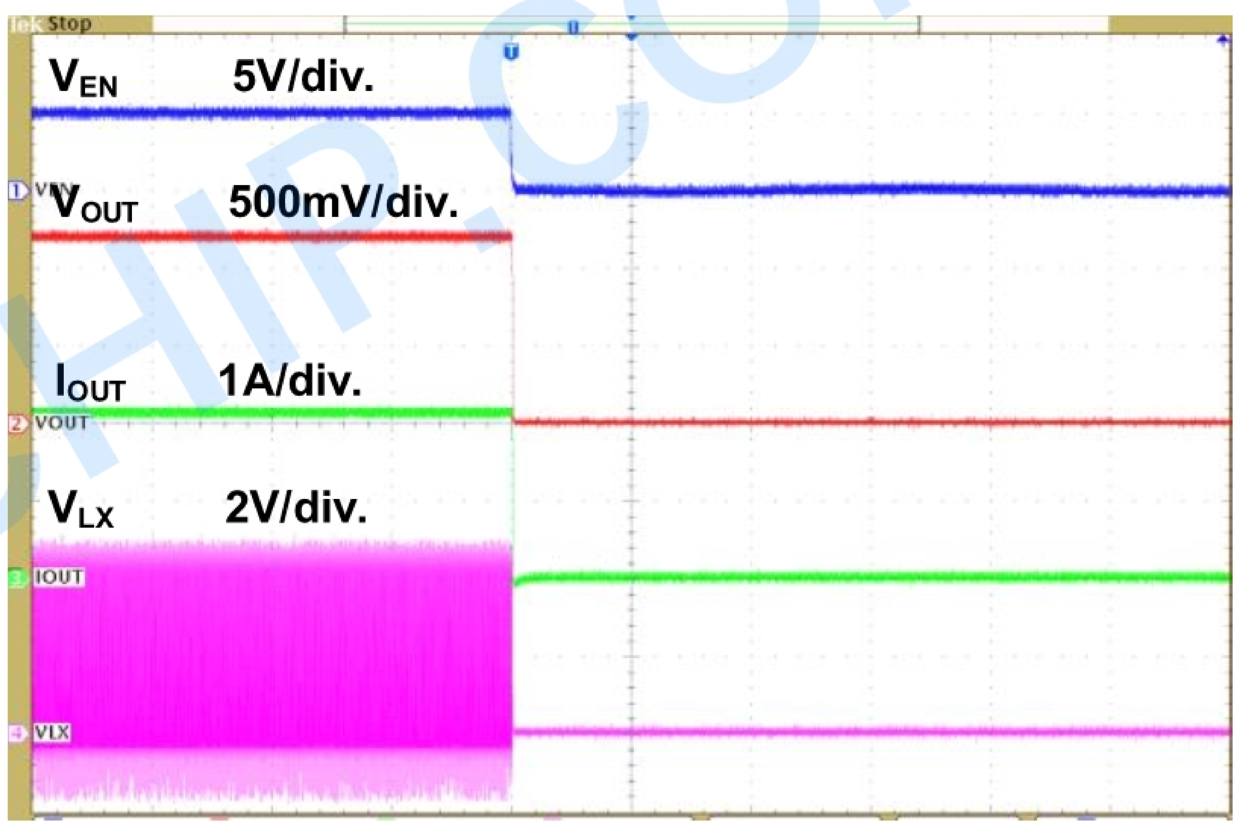
I_{OUT}=0A



4ms/div.

Power Off through EN Waveform

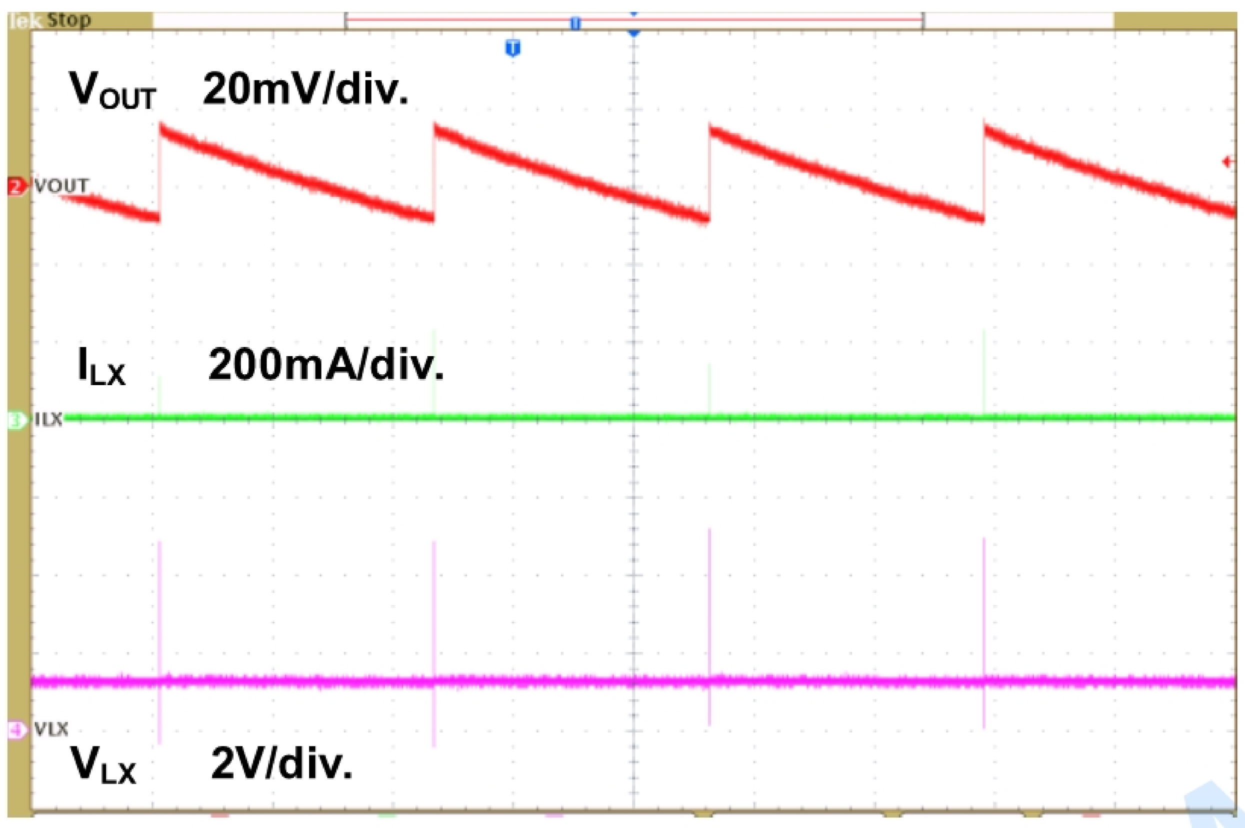
I_{OUT}=2A



4ms/div.

Power Off through EN Waveform

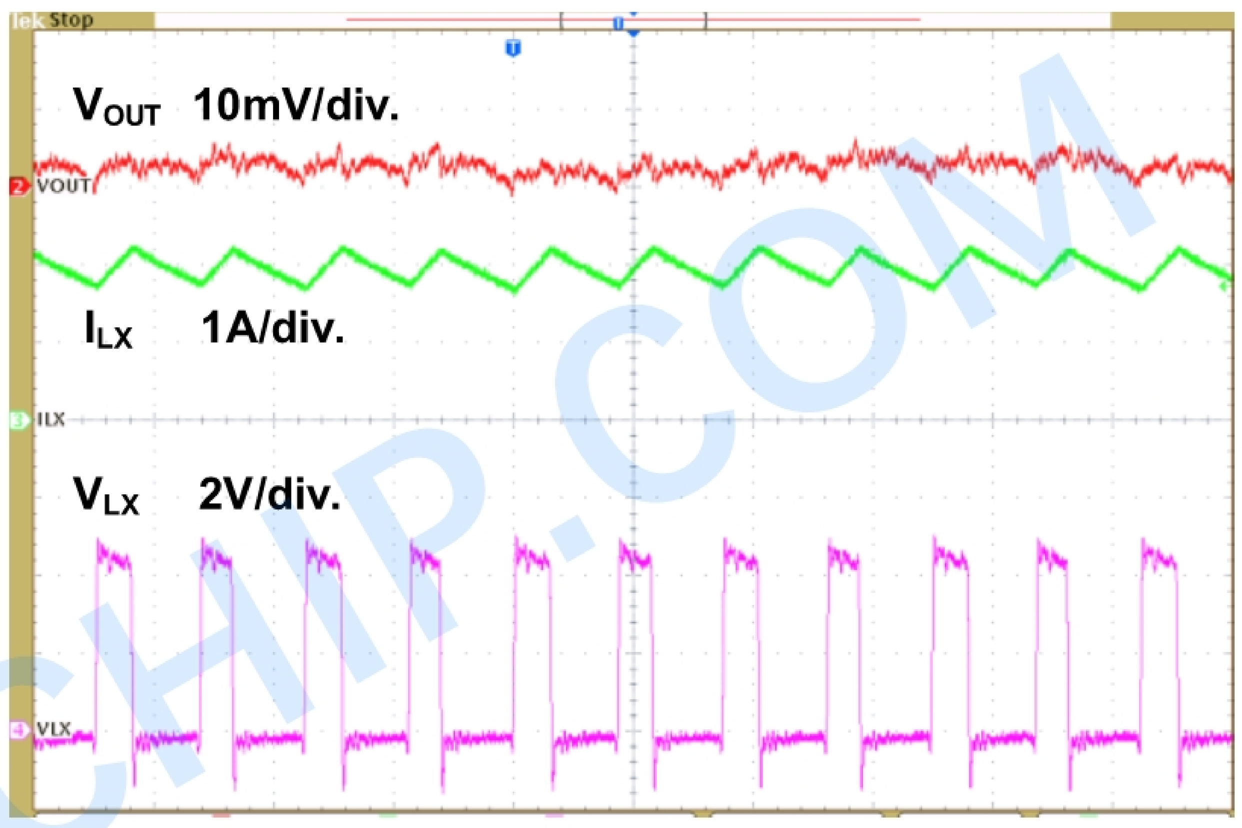
I_{OUT}=0A



20ms/div

Steady State Waveform

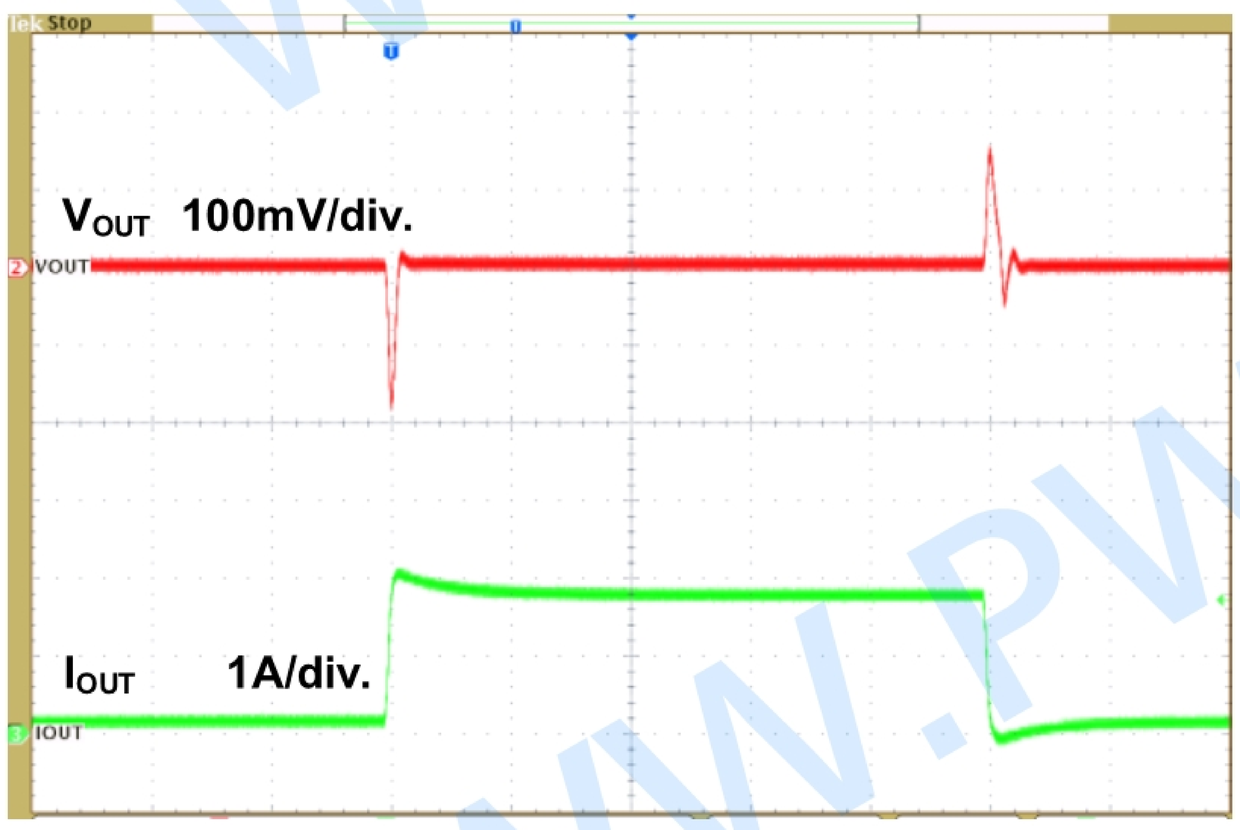
I_{OUT}=2A



1μs/div

Steady State Waveform

I_{OUT}=0.2A to 2A



200μs/div.

Load Transient Waveform

Function Description

The PW2052 is a high efficiency, internal compensation and constant frequency current mode step-down synchronous DC/DC converter. It has integrated high-side (180mΩ, typ) and low-side (100mΩ, typ) power switches, and provides 2A continuous load current. It regulates input voltage from 2.5V to 5.5V, and down to an output voltage as low as 0.6V

Control Loop

Slope compensated current mode PWM control provides stable switching and cycle-by-cycle current limit for superior load, line response, protection of the internal main switch and synchronous rectifier. The PW2052 switches at a constant frequency (1MHz) and regulates the output voltage. During each cycle, the PWM comparator modulates the power transferred to the load by changing the inductor peak current based on the feedback error voltage. During normal operation, the main switch is turned on for a certain time to ramp the inductor current at each rising edge of the internal oscillator, and switched off when the peak inductor current is above the error voltage. When the main switch is off, the synchronous rectifier will be turned on immediately and stay on until next cycle starts.

Enable

The PW2052 CE pin provides digital control to turn on/off the regulator. When the voltage of CE exceeds the threshold voltage, the regulator will start the soft start function. If the CE pin voltage is below the shutdown threshold voltage, the regulator will turn into the shutdown mode and the shutdown current will be smaller than 1μA. For auto start-up operation, connect CE to VIN.

Soft-Start

The PW2052 employs internal soft-start function to reduce input inrush current during start up. The internal soft start time will be 1ms.

Under Voltage Lockout

When the PW2052 is power on, the internal circuits will be held inactive until VIN voltage exceeds the UVLO threshold voltage. And the regulator will be disabled when VIN is below the UVLO threshold voltage. The hysteretic of the UVLO comparator is 200mV (typ).

Short Circuit Protection

The PW2052 provides short circuit protection function to prevent the device damaged from short condition. When the short condition occurs and the feedback voltage drops lower than 40% of the regulation level, this will activate the latch protection circuit. Then output will be forced shutdown to prevent the inductor current runaway and to reduce the power dissipation within the IC under true short circuit conditions. Once the short condition is removed, reset EN or VIN to restart IC.

Over Current Protection

The PW2052 over current protection function is implemented by using cycle-by-cycle current limit architecture. The inductor current is monitored by measuring the high-side MOSFET series sense resistor voltage. When the load current increases, the inductor current will also increase. When the peak inductor current reaches the current limit threshold, the output voltage will start to drop. When the over current condition is removed, the output voltage will return to the regulated value.

Over Temperature Protection

The PW2051 incorporates an over temperature protection circuit to protect itself from overheating. When the junction temperature exceeds the thermal shutdown threshold temperature, the regulator will be shutdown. And the hysteretic of the over temperature protection is 30°C (typ).

Application Information

Output Voltage Setting

The output voltage VOUT is set by using a resistive divider from the output to FB. The FB pin regulated voltage is 0.6V. Thus the output voltage is:

$$\left(1+\frac{R1}{R2}\right)*0.6V=Vout$$

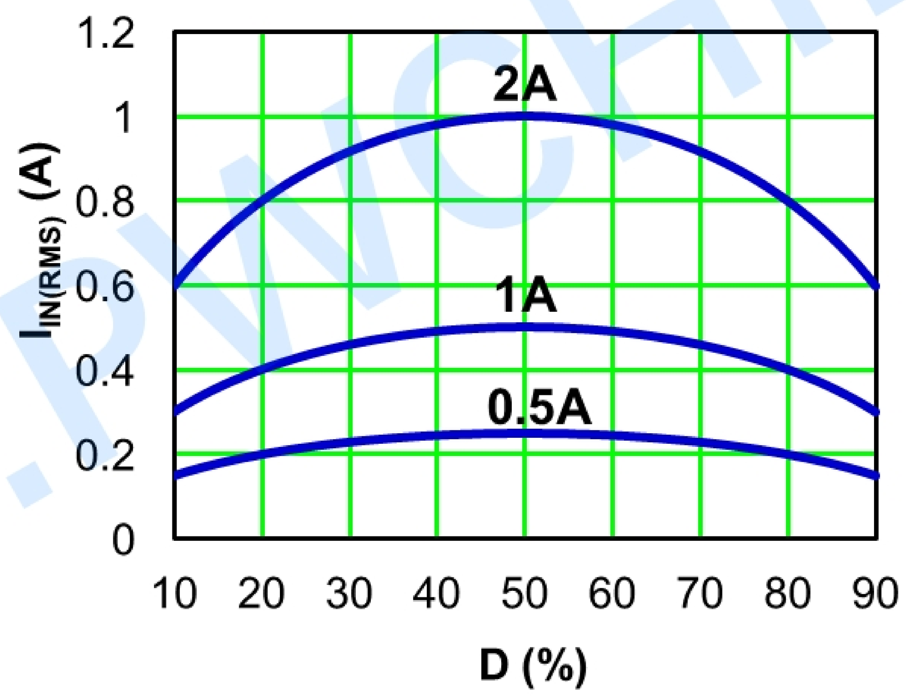
Input Capacitor Selection

The use of the input capacitor is filtering the input voltage ripple and the MOSFETS switching spike voltage. Because the input current to the step-down converter is discontinuous, the input capacitor is required to supply the current to the converter to keep the DC input voltage. The capacitor voltage rating should be 1.25 to 1.5 times greater than the maximum input voltage. The input capacitor ripple current RMS value is calculated as:

$$I_{IN(RMS)}=I_{OUT}\times\sqrt{D\times(1-D)}$$

$$D=\frac{V_{OUT}}{V_{IN}}$$

Where D is the duty cycle of the power MOSFET. This function reaches the maximum value at D=0.5 and the equivalent RMS current is equal to IOUT/2. The following diagram is the graphical representation of above equation.



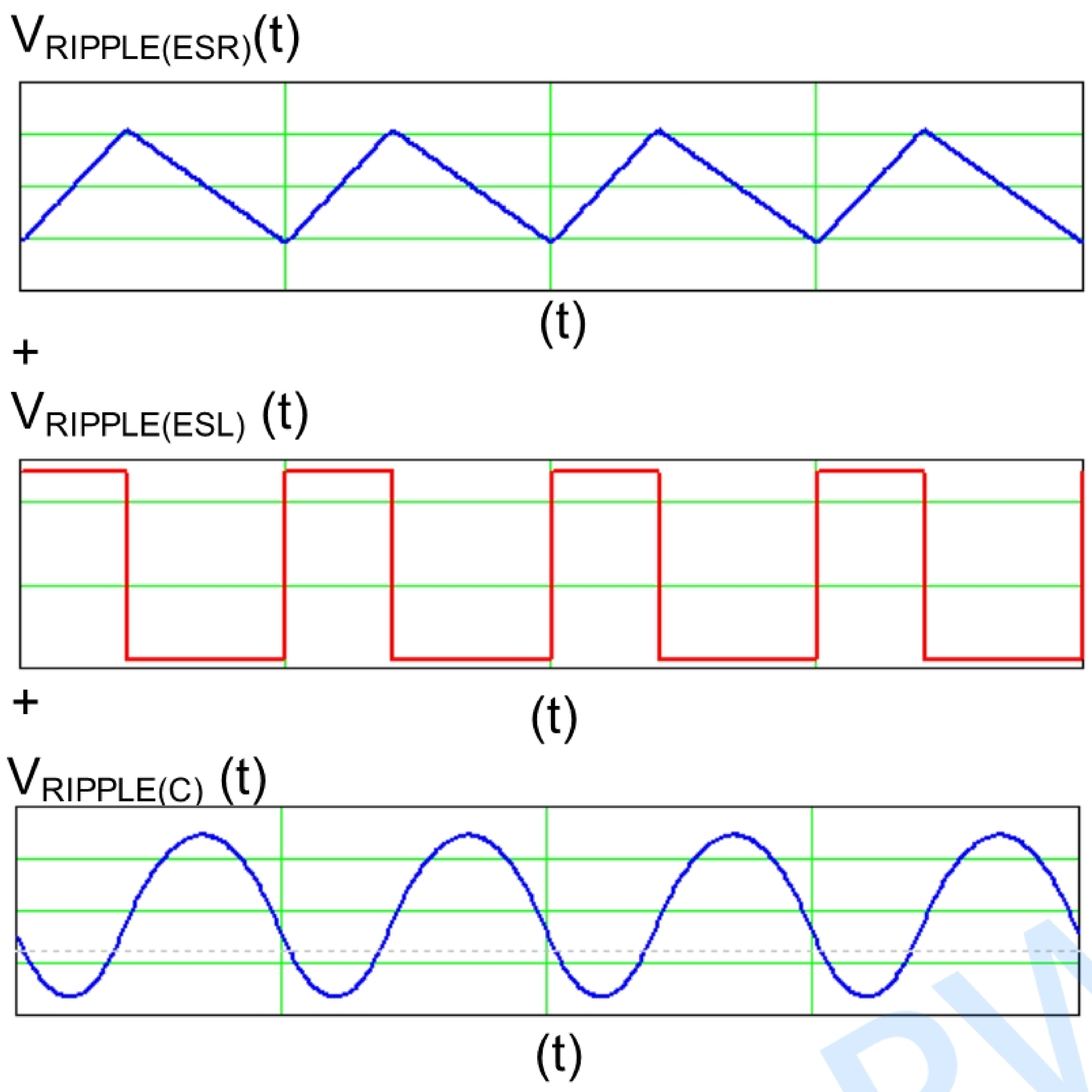
A low ESR capacitor is required to keep the noise minimum. Ceramic capacitors are better, but tantalum or low ESR electrolytic capacitors may also suffice.

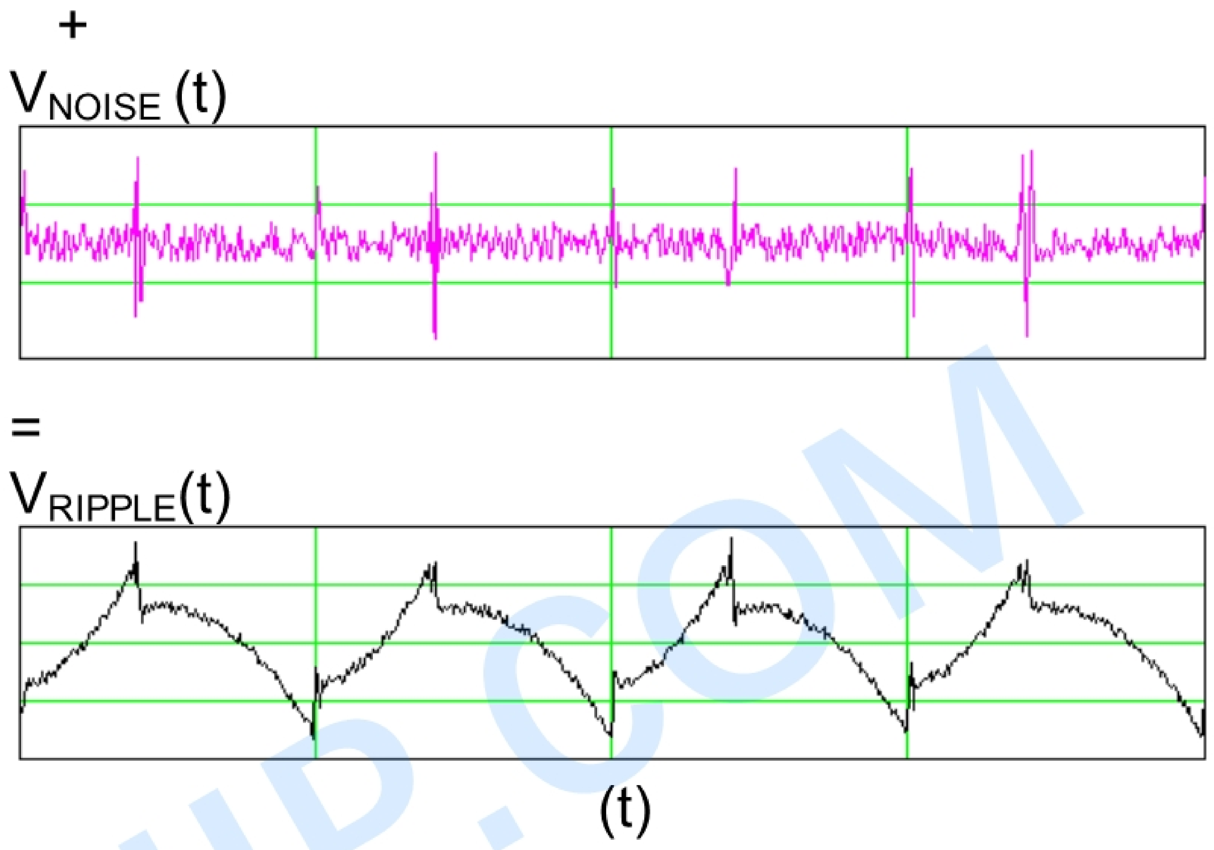
Output Capacitor Selection

The output capacitor is used to keep the DC output voltage and supply the load transient current. When operating in constant current mode, the output ripple is determined by four components:

$$V_{RIPPLE}(t)=V_{RIPPLE(C)}(t)+V_{RIPPLE(ESR)}(t)+V_{RIPPLE(ESL)}(t)+V_{NOISE}(t)$$

The following figures show the form of the ripple contributions.





$$V_{RIPPLE(ESR)}=\frac{V_{OUT}}{F_{OSC}\times L}\times\left(1-\frac{V_{OUT}}{V_{IN}}\right)\times ESR$$

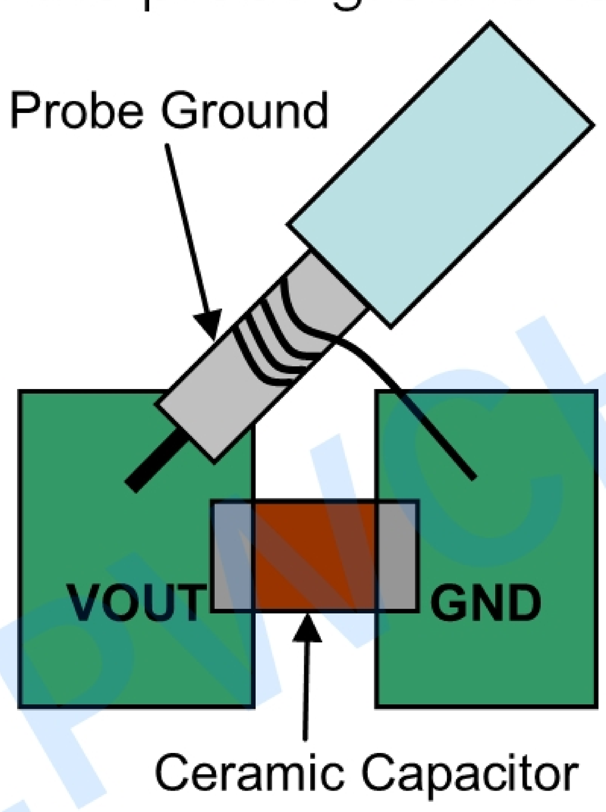
$$V_{RIPPLE(ESL)}=\frac{ESL}{L+ESL}\times V_{IN}$$

$$V_{RIPPLE(C)}=\frac{V_{OUT}}{8\times F_{OSC}{}^{2}\times L\times C_{OUT}}\times\left(1-\frac{V_{OUT}}{V_{IN}}\right)$$

Where FOSC is the switching frequency, L is the inductance value, VIN is the input voltage, ESR is the equivalent series resistance value of the output capacitor, ESL is the equivalent series inductance value of the output capacitor and the COUT is the output capacitor.

Low ESR capacitors are preferred to use. Ceramic, tantalum or low ESR electrolytic capacitors can be used depending on the output ripple requirements. When using the ceramic capacitors, the ESL component is usually negligible.

It is important to use the proper method to eliminate high frequency noise when measuring the output ripple. The figure shows how to locate the probe across the capacitor when measuring output ripple. Remove the scope probe plastic jacket in order to expose the ground at the tip of the probe. It gives a very short connection from the probe ground to the capacitor and eliminates noise



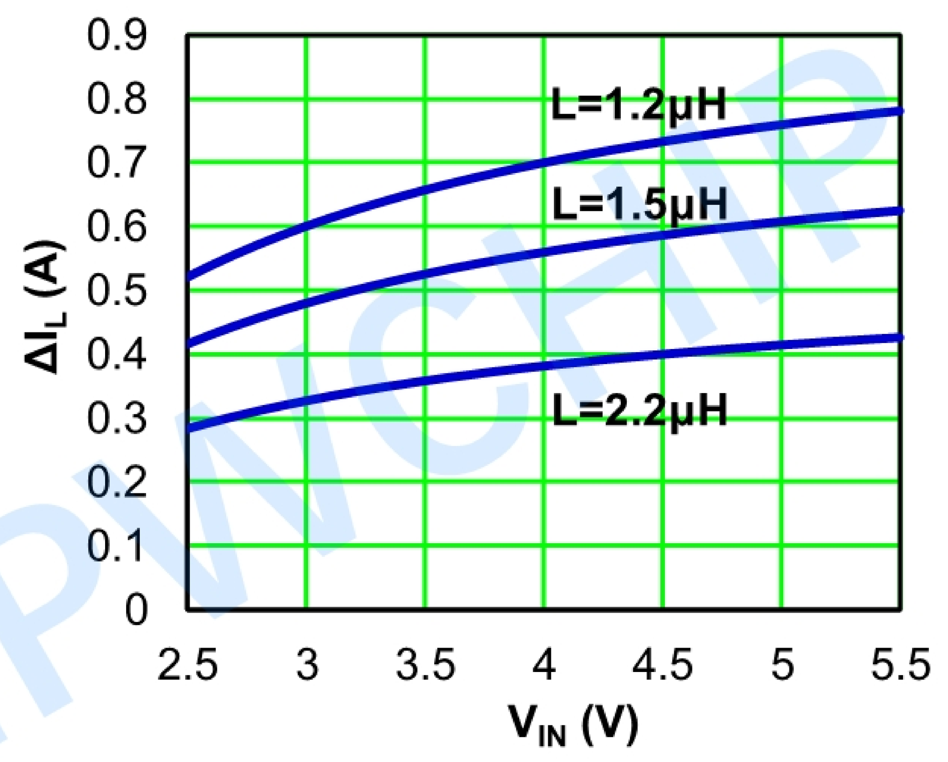
Inductor Selection

The output inductor is used for storing energy and filtering output ripple current. But the trade-off condition often happens between maximum energy storage and the physical size of the inductor. The first consideration for selecting the output inductor is to make sure that the inductance is large enough to keep the converter in the continuous current mode.

That will lower ripple current and result in lower output ripple voltage. The Δ L is inductor peak-to-peak ripple current:

$$\Delta I_L = \frac{V_{OUT}}{F_{OSC} \times L} \times \left(1 - \frac{V_{OUT}}{V_{IN}}\right)$$

The following diagram is an example to graphically represent Δ IL equation.



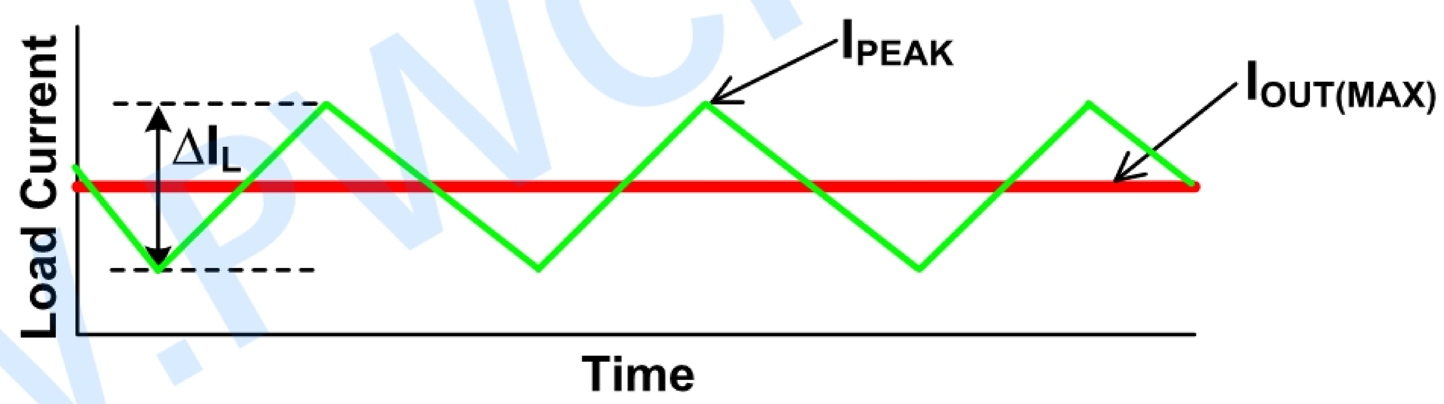
A good compromise value between size and efficiency is to set the peak-to-peak inductor ripple current Δ IL equal to 30% of the maximum load current. But setting the peak-to-peak inductor ripple current ΔIL between 20%~50% of the maximum load current is also acceptable. Then the inductance can be calculated with the following equation:

$$\Delta I_L = 0.3 \times I_{OUT(MAX)}$$

$$L = \frac{(V_{IN} - V_{OUT}) \times V_{OUT}}{V_{IN} \times F_{OSC} \times \Delta I_L}$$

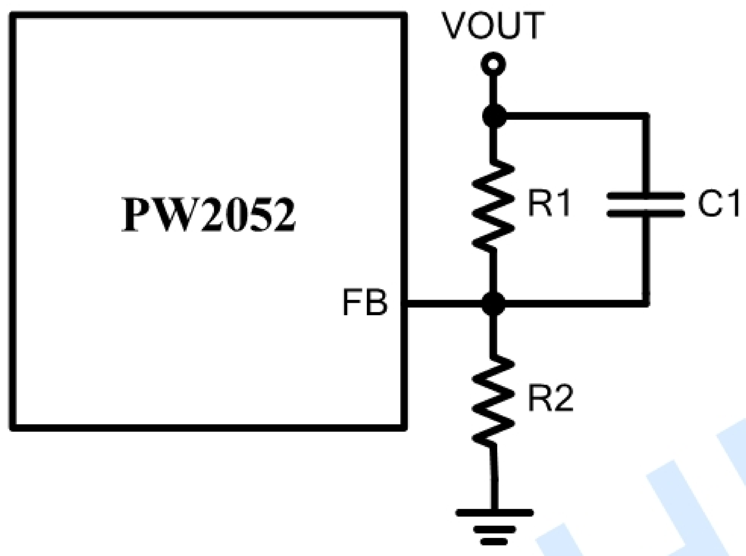
To guarantee sufficient output current, peak inductor current must be lower than the PW2052 high-side MOSFET current limit. The peak inductor current is shown as below:

$$I_{PEAK} = I_{OUT(MAX)} + \frac{\Delta I_L}{2}$$



Feedforward Capacitor Selection

Internal compensation function allows users saving time in design and saving cost by reducing the number of external components. The use of a feedforward capacitor C1 in the feedback network is recommended to improve transient response or higher phase margin.



For optimizing the feedforward capacitor, knowing the cross frequency is the first thing. The cross frequency (or the converter bandwidth) can be determined by using a network analyzer. When getting the cross frequency with no feedforward capacitor identified, the value of feedforward capacitor C1 can be calculated with the following equation:

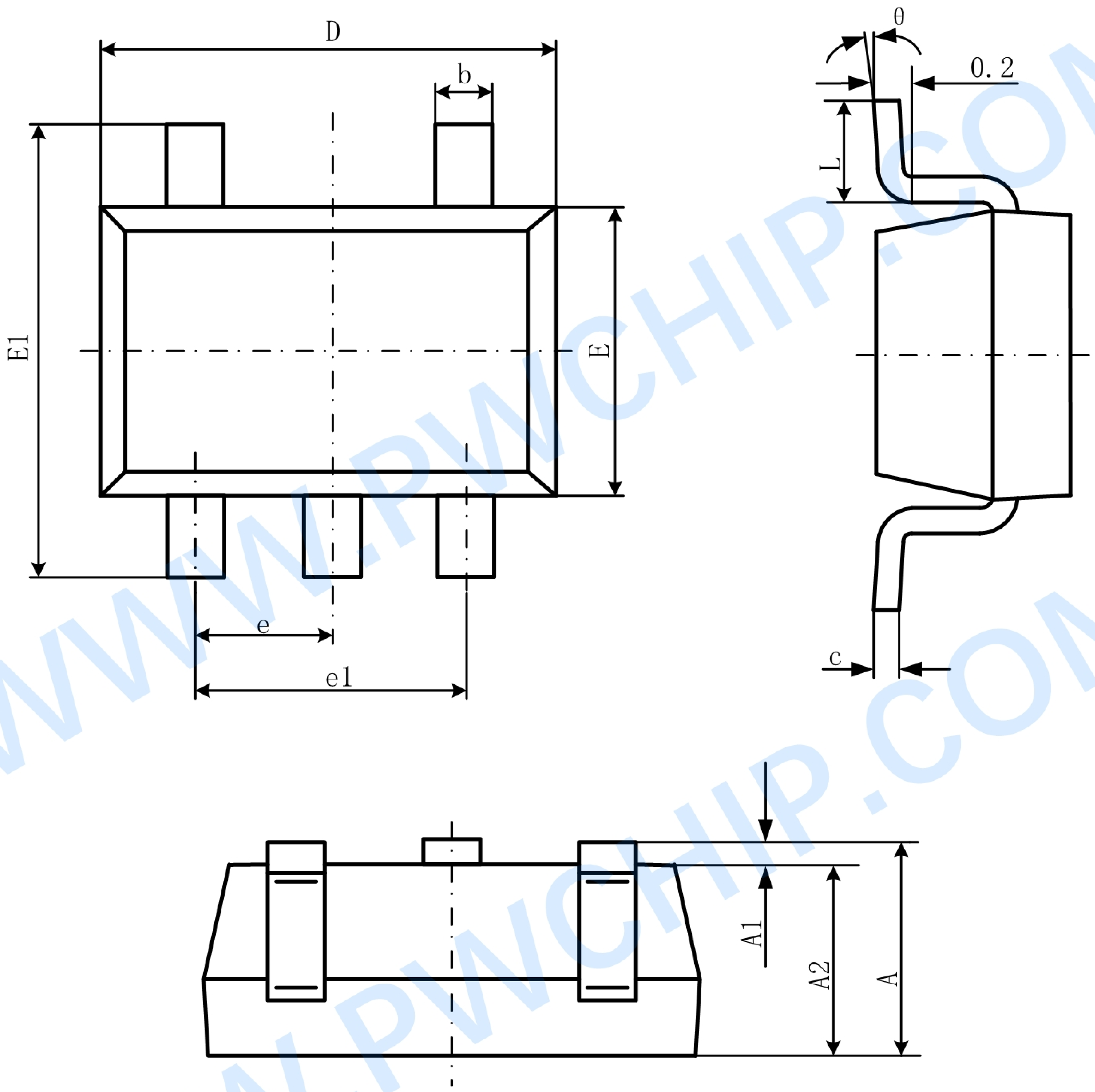
$$C1 \quad \frac{1}{2\pi \times F_{CROSS}} \times \sqrt{\frac{1}{R1} \times \left(\frac{1}{R1} + \frac{1}{R2}\right)}$$

Where FCROSS is the cross frequency.

To reduce transient ripple, the feedforward capacitor value can be increased to push the cross frequency to higher region. Although this can improve transient response, it also decreases phase margin and causes more ringing. In the other hand, if more phase margin is desired, the feedforward capacitor value can be decreased to push the cross frequency to lower region. In general, the feedforward capacitor range is between 10pF to 330pF.

PACKAGE DESCRIPTION

SOT23-5L



Symbol	Dimensions In Millimeters	
	Min	Max
A	0.900	1.450
A1	0.000	0.150
A2	0.900	1.300
b	0.300	0.500
c	0.100	0.200
D	2.800	3.000
E	1.500	1.700
E1	2.650	2.950
e	0.950(BSC)	
e1	1.800	2.000
L	0.300	0.600
θ	0°	8°

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